

# OPA1612-Q1 SoundPlus High-Performance, Bipolar-Input Audio Operational Amplifier

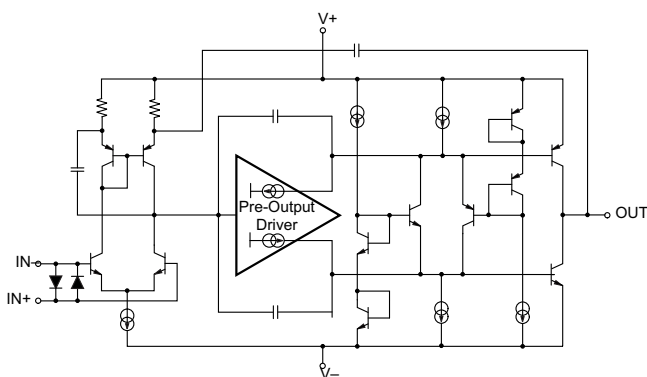
## 1 Features

- Qualified for Automotive Applications
- AEC-Q100 Qualified With the Following Results:
  - Device Temperature Grade 1:  $-40^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$  Ambient Operating Temperature Range
  - Device HBM Classification Level 2
  - Device CDM Classification Level C6
- Superior Sound Quality
- Ultralow Noise:  $1.1\text{ nV}/\sqrt{\text{Hz}}$  at 1 kHz
- Ultralow Distortion: 0.000015% at 1 kHz
- High Slew Rate:  $27\text{ V}/\mu\text{s}$
- Wide Bandwidth: 40 MHz ( $G = +1$ )
- High Open-Loop Gain: 130 dB
- Unity Gain Stable
- Low Quiescent Current: 3.6 mA per Channel
- Rail-to-Rail Output
- Wide Supply Range:  $\pm 2.25\text{ V}$  to  $\pm 18\text{ V}$

## 2 Applications

- Professional Audio Equipment
- Microphone Preamplifiers
- Analog and Digital Mixing Consoles
- Broadcast Studio Equipment
- Audio Test And Measurement
- High-End A/V Receivers

**Functional Block Diagram**



## 3 Description

The OPA1612-Q1 device is a dual, SoundPlus™, bipolar-input operational amplifier that achieves very low  $1.1\text{ nV}/\sqrt{\text{Hz}}$  noise density with an ultralow distortion of 0.000015% at 1 kHz. The OPA1612-Q1 device offers rail-to-rail output swing to within 600 mV with a 2-k $\Omega$  load, which increases headroom and maximizes dynamic range. These devices also have a high output drive capability of  $\pm 30\text{ mA}$ .

These devices operate over a very wide supply range of  $\pm 2.25\text{ V}$  to  $\pm 18\text{ V}$ , on only 3.6 mA of supply current per channel. The OPA1612-Q1 op amp is unity-gain stable and provide excellent dynamic behavior over a wide range of load conditions.

The dual version features completely independent circuitry for lowest crosstalk and freedom from interactions between channels, even when overdriven or overloaded.

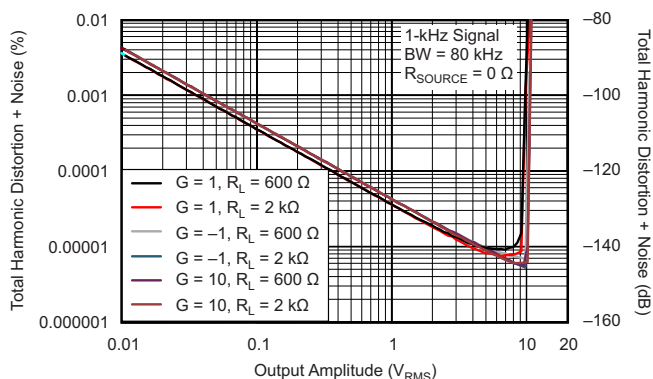
The OPA1612-Q1 device is available in a SOIC-8 package. The device is specified from  $-40^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$ .

**Device Information<sup>(1)</sup>**

PART NUMBER	PACKAGE	BODY SIZE (NOM)
OPA1612-Q1	SOIC (8)	4.90 mm x 3.91 mm

(1) For all available packages, see the orderable addendum at the end of the datasheet.

**THD+N Ratio vs Output Amplitude**



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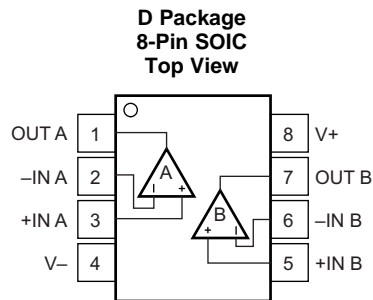
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## 4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

<b>Changes from Original (November 2015) to Revision A</b>	<b>Page</b>
• Changed the device status from <i>Product Preview</i> to <i>Production Data</i> .....	<b>1</b>

## 5 Pin Configuration and Functions



**Pin Functions**

PIN		I/O	DESCRIPTION
NO.	NAME		
1	OUT A	O	Output, channel A
2	-IN A	I	Inverting input, channel A
3	+IN A	I	Noninverting input, channel A
4	V-	—	Negative (lowest) power supply
5	+IN B	I	Inverting input, channel B
6	-IN B	I	Noninverting input, channel B
7	OUT B	O	Output, channel B
8	V+	—	Positive (highest) power supply

## 6 Specifications

### 6.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted)<sup>(1)</sup>

		MIN	MAX	UNIT
$V_S$ <sup>(2)</sup>	Supply voltage		40	V
	Input voltage	(V-) - 0.5	(V+) + 0.5	V
	Input current (all pins except power-supply pins)		±10	mA
	Output short-circuit <sup>(2)</sup>	Continuous		
$T_A$	Operating temperature	-55	125	°C
$T_J$	Junction temperature		200	°C
$T_{stg}$	Storage temperature	-65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) Short-circuit to  $V_S / 2$  (ground in symmetrical dual supply setups), one amplifier per package.

### 6.2 ESD Ratings

		VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human-body model (HBM), per AEC Q100-002 <sup>(1)</sup>	±3000
		Charged-device model (CDM), per AEC Q100-011	±1000

- (1) AEC Q100-002 indicates that HBM stressing shall be in accordance with the ANSI/ESDA/JEDEC JS-001 specification.

### 6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

	MIN	NOM	MAX	UNIT
Supply voltage (V+ - V-)	4.5 (±2.25)		36 (±18)	V
Specified temperature	-40		85	°C

### 6.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>	OPA1612-Q1		UNIT	
	D (SOIC)			
	8 PINS			
$R_{\theta JA}$	Junction-to-ambient thermal resistance		111.9	°C/W
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance		26.5	°C/W
$R_{\theta JB}$	Junction-to-board thermal resistance		0.8	°C/W
$\Psi_{JT}$	Junction-to-top characterization parameter		20.9	°C/W
$\Psi_{JB}$	Junction-to-board characterization parameter		1.6	°C/W
$R_{\theta JC(bot)}$	Junction-to-case (bottom) thermal resistance		—	°C/W

- (1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, [SPRA953](#).

## 6.5 Electrical Characteristics: $V_S = \pm 2.25\text{ V to } \pm 18\text{ V}$

At  $T_A = 25^\circ\text{C}$  and  $R_L = 2\text{ k}\Omega$ , unless otherwise noted.  $V_{CM} = V_{OUT} = \text{midsupply}$ , unless otherwise noted.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>AUDIO PERFORMANCE</b>						
THD+N	Total harmonic distortion + noise	$G = +1$ , $f = 1\text{ kHz}$ , $V_O = 3 V_{RMS}$	0.000015%			
				-136		dB
IMD	Intermodulation distortion	SMPTE/DIN two-tone, 4:1 (60 Hz and 7 kHz), $G = +1$ , $V_O = 3 V_{RMS}$	0.000015%			
				-136		dB
		DIM 30 (3-kHz square wave and 15-kHz sine wave), $G = +1$ , $V_O = 3 V_{RMS}$	0.000012%			
				-138		dB
		CCIF twin-tone (19 kHz and 20 kHz), $G = +1$ , $V_O = 3 V_{RMS}$	0.000008%			
				-142		dB
<b>FREQUENCY RESPONSE</b>						
GBW	Gain-bandwidth product	$G = 100$		80		MHz
		$G = 1$		40		MHz
SR	Slew rate	$G = -1$		27		V/ $\mu\text{s}$
		Full-power bandwidth <sup>(1)</sup>	$V_O = 1 V_{PP}$	4		MHz
	Overload recovery time	$G = -10$		500		ns
	Channel separation (dual)	$f = 1\text{ kHz}$		-130		dB
<b>NOISE</b>						
	Input voltage noise	$f = 20\text{ Hz to } 20\text{ kHz}$		1.2		$\mu\text{V}_{PP}$
$e_n$	Input voltage noise density <sup>(2)</sup>	$f = 10\text{ Hz}$		2		$\text{nV}/\sqrt{\text{Hz}}$
		$f = 100\text{ Hz}$		1.5		$\text{nV}/\sqrt{\text{Hz}}$
		$f = 1\text{ kHz}$		1.1	1.5	$\text{nV}/\sqrt{\text{Hz}}$
$i_n$	Input current noise density	$f = 10\text{ Hz}$		3		$\text{pA}/\sqrt{\text{Hz}}$
		$f = 1\text{ kHz}$		1.7		$\text{pA}/\sqrt{\text{Hz}}$
<b>OFFSET VOLTAGE</b>						
$V_{OS}$	Input offset voltage	$V_S = \pm 15\text{ V}$		$\pm 100$	$\pm 500$	$\mu\text{V}$
$dV_{OS}/dT$	$V_{OS}$ over temperature <sup>(2)</sup>	$T_A = -40^\circ\text{C to } +125^\circ\text{C}$		1	4	$\mu\text{V}/^\circ\text{C}$
PSRR	Power-supply rejection ratio	$V_S = \pm 2.25\text{ V to } \pm 18\text{ V}$		0.1	1	$\mu\text{V}/\text{V}$
<b>INPUT BIAS CURRENT</b>						
$I_B$	Input bias current	$V_{CM} = 0\text{ V}$		$\pm 60$	$\pm 250$	nA
		$V_{CM} = 0\text{ V}$ , DRG package only		$\pm 60$	$\pm 300$	nA
	$I_B$ over temperature <sup>(2)</sup>	$T_A = -40^\circ\text{C to } +125^\circ\text{C}$			350	nA
$I_{OS}$	Input offset current	$V_{CM} = 0\text{ V}$		$\pm 25$	$\pm 175$	nA
<b>INPUT VOLTAGE RANGE</b>						
$V_{CM}$	Common-mode voltage range		$(V-) + 2$		$(V+) - 2$	V
CMRR	Common-mode rejection ratio	$(V-) + 2\text{ V} \leq V_{CM} \leq (V+) - 2\text{ V}$	110	120		dB
<b>INPUT IMPEDANCE</b>						
	Differential			20k    8		$\Omega$    pF
	Common-mode			$10^9$    2		$\Omega$    pF

(1) Full-power bandwidth =  $SR / (2\pi \times V_P)$ , where SR = slew rate.

(2) Specified by design and characterization.

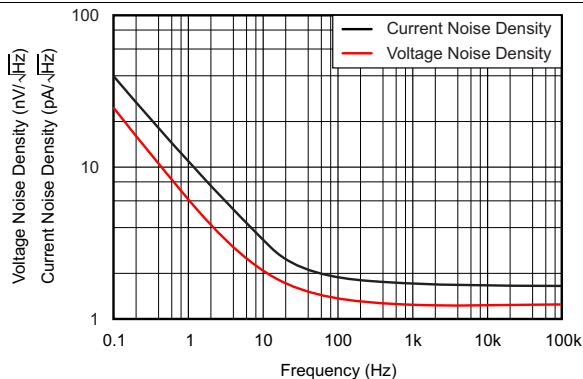
**Electrical Characteristics:  $V_S = \pm 2.25\text{ V}$  to  $\pm 18\text{ V}$  (continued)**

 At  $T_A = 25^\circ\text{C}$  and  $R_L = 2\text{ k}\Omega$ , unless otherwise noted.  $V_{CM} = V_{OUT} = \text{midsupply}$ , unless otherwise noted.

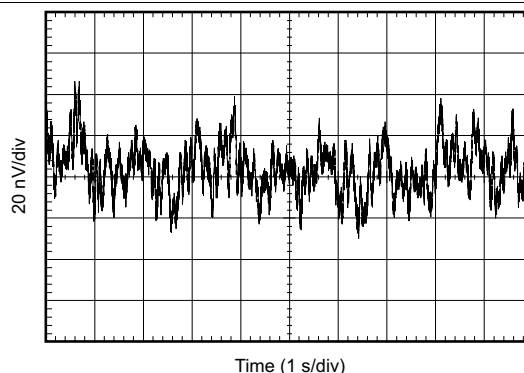
PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>OPEN-LOOP GAIN</b>						
$A_{OL}$	Open-loop voltage gain	$(V^-) + 0.2\text{ V} \leq V_O \leq (V^+) - 0.2\text{ V}$ , $R_L = 10\text{ k}\Omega$	114	130		dB
		$(V^-) + 0.6\text{ V} \leq V_O \leq (V^+) - 0.6\text{ V}$ , $R_L = 2\text{ k}\Omega$	110	114		dB
<b>OUTPUT</b>						
$V_{OUT}$	Voltage output	$R_L = 10\text{ k}\Omega$ , $A_{OL} \geq 114\text{ dB}$	$(V^-) + 0.2$		$(V^+) - 0.2$	V
		$R_L = 2\text{ k}\Omega$ , $A_{OL} \geq 110\text{ dB}$	$(V^-) + 0.6$		$(V^+) - 0.6$	V
$I_{OUT}$	Output current		See <a href="#">Figure 27</a>			mA
$Z_O$	Open-loop output impedance		See <a href="#">Figure 28</a>			$\Omega$
$I_{SC}$	Short-circuit current	Source, $V_S = \pm 18\text{ V}$	55			mA
		Sink, $V_S = \pm 18\text{ V}$	-62			mA
$C_{LOAD}$	Capacitive load drive		See <a href="#">Typical Characteristics</a>			pF
<b>POWER SUPPLY</b>						
$V_S$	Specified voltage		$\pm 2.25$		$\pm 18$	V
$I_Q$	Quiescent current (per channel)	$I_{OUT} = 0\text{ A}$		3.6	4.5	mA
	$I_Q$ over Temperature <sup>(2)</sup>	$T_A = -40^\circ\text{C}$ to $+125^\circ\text{C}$			5.5	mA
<b>TEMPERATURE RANGE</b>						
	Specified range		-40		125	$^\circ\text{C}$
	Operating range		-55		125	$^\circ\text{C}$

## 6.6 Typical Characteristics

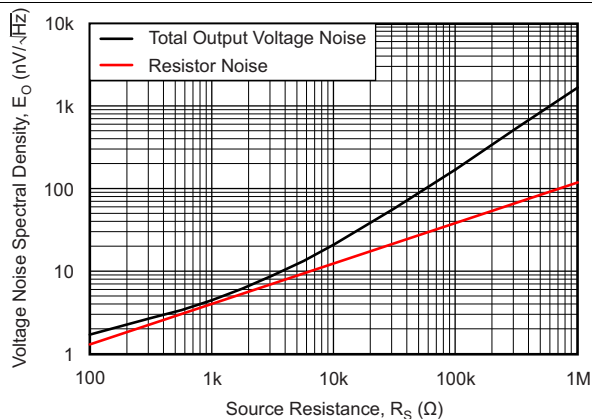
At  $T_A = 25^\circ$ ,  $V_S = \pm 15$  V, and  $R_L = 2$  k $\Omega$ , unless otherwise noted.



**Figure 1. Input Voltage Noise Density and Input Current Noise Density vs Frequency**

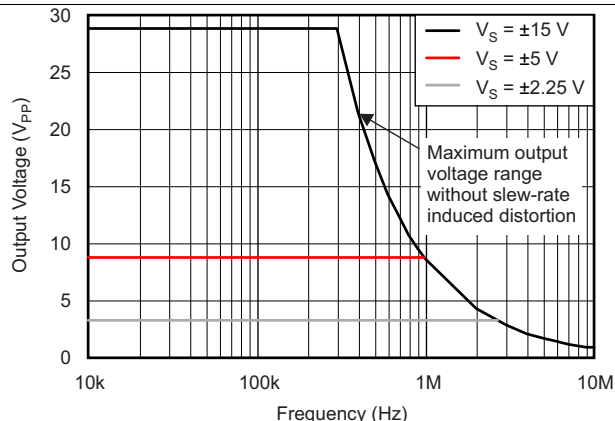


**Figure 2. 0.1-Hz to 10-Hz Noise**

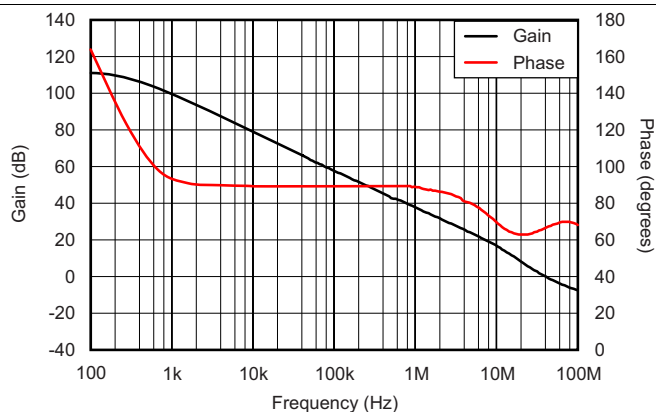


$$E_O^2 = e_n^2 + (i_n \times R_S)^2 + 4kRT_S \quad \text{See Figure 29}$$

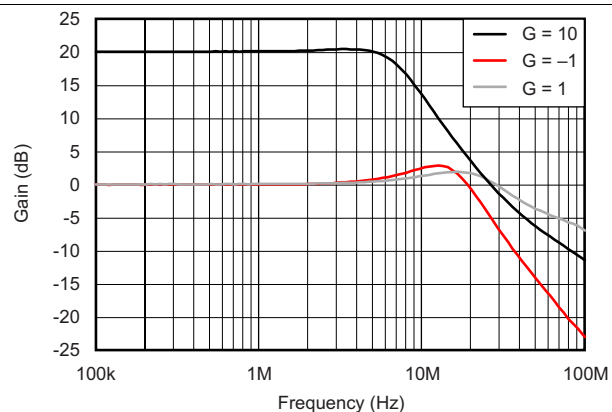
**Figure 3. Voltage Noise vs Source Resistance**



**Figure 4. Maximum Output Voltage vs Frequency**



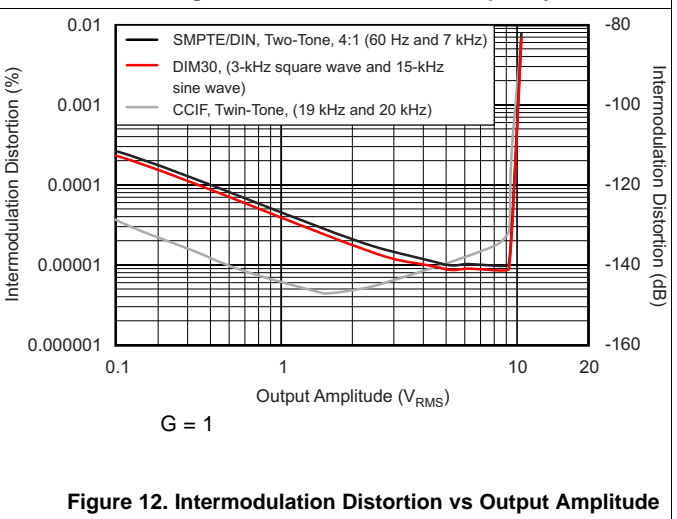
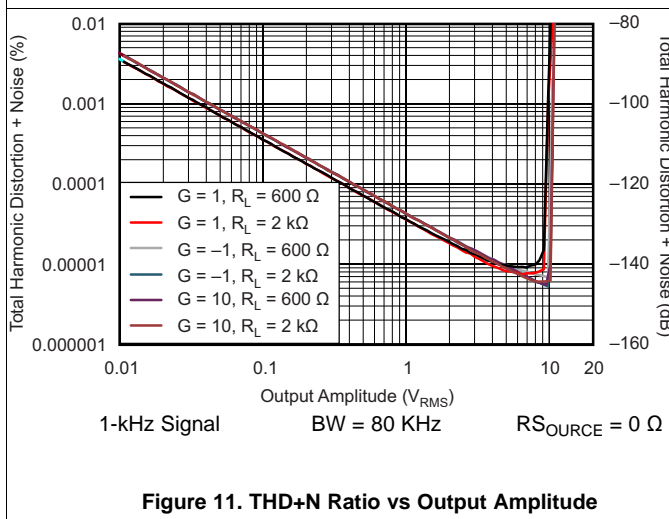
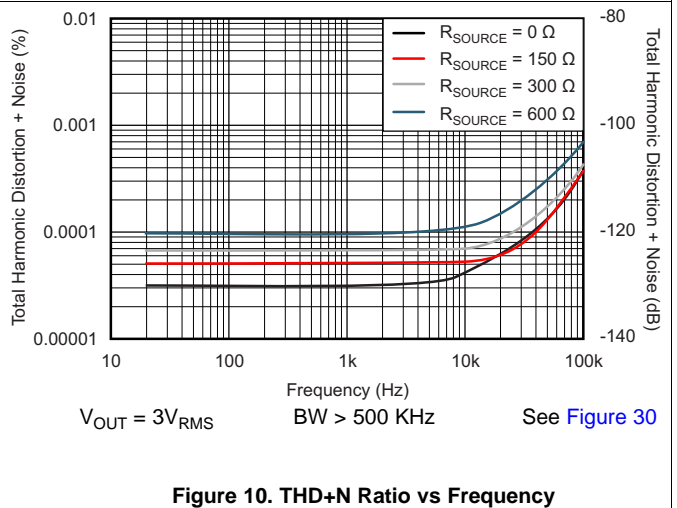
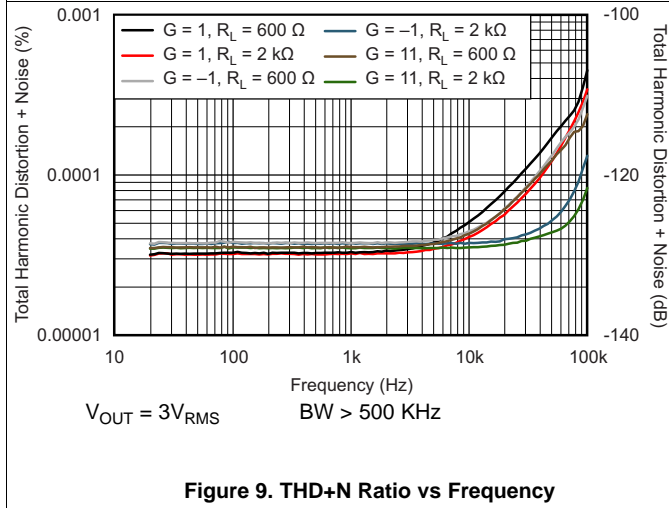
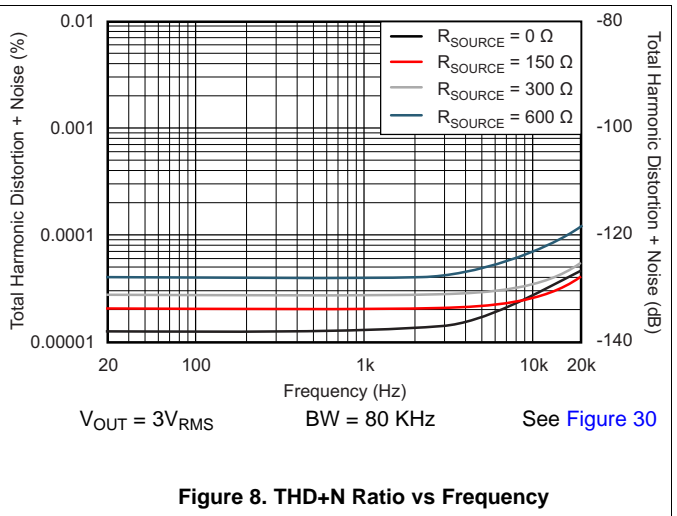
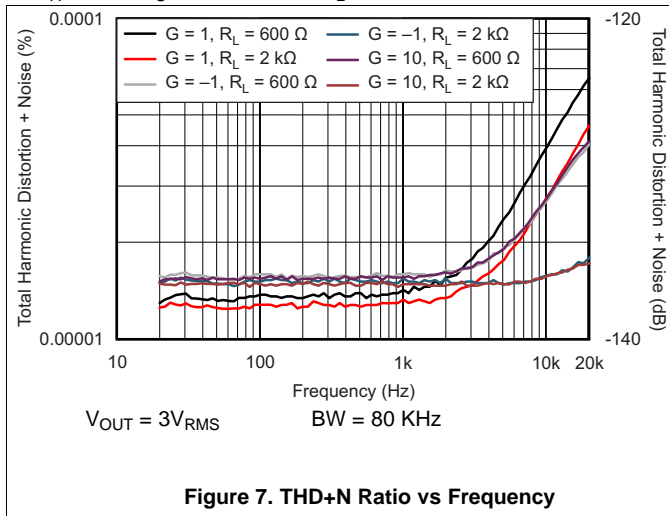
**Figure 5. Gain and Phase vs Frequency**



**Figure 6. Closed-Loop Gain vs Frequency**

Typical Characteristics (continued)

At  $T_A = 25^\circ$ ,  $V_S = \pm 15$  V, and  $R_L = 2$  k $\Omega$ , unless otherwise noted.





### Typical Characteristics (continued)

At  $T_A = 25^\circ$ ,  $V_S = \pm 15$  V, and  $R_L = 2$  k $\Omega$ , unless otherwise noted.

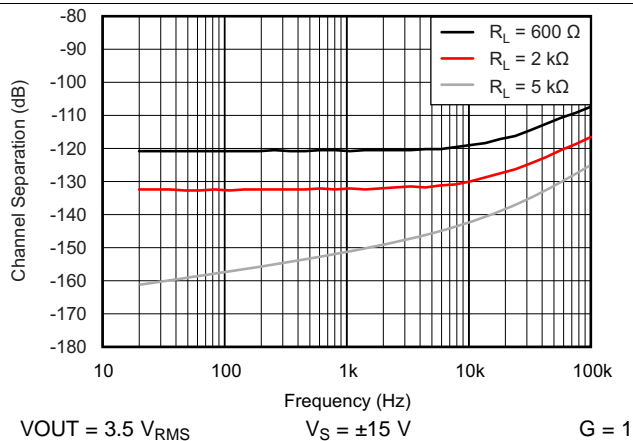


Figure 13. Channel Separation vs Frequency

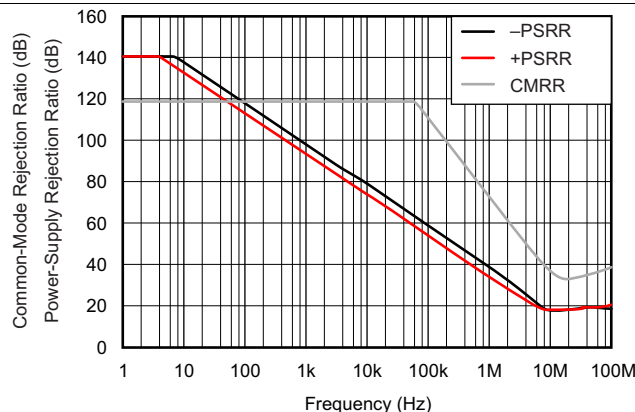


Figure 14. CMRR and PSRR vs Frequency (Referred to Input)

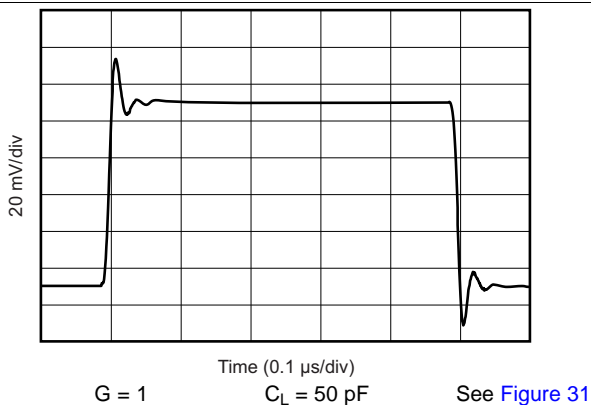


Figure 15. Small-Signal Step Response (100 mV)

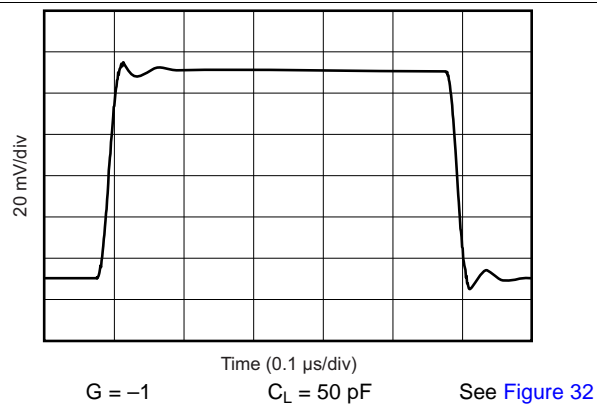


Figure 16. Small-Signal Step Response (100 mV)

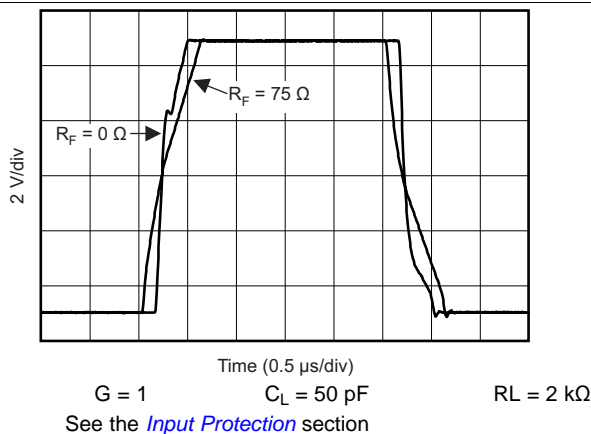


Figure 17. Large-Signal Step Response

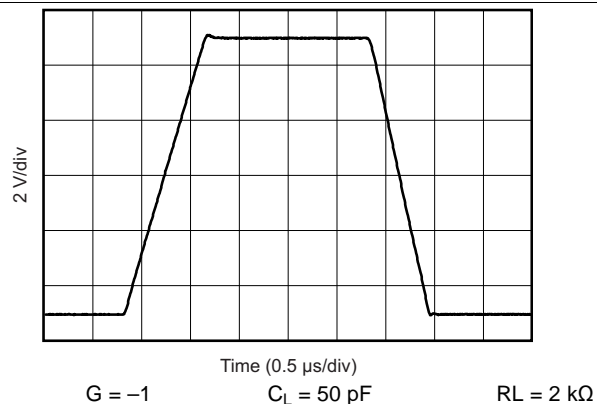


Figure 18. Large-Signal Step Response

Typical Characteristics (continued)

At  $T_A = 25^\circ$ ,  $V_S = \pm 15$  V, and  $R_L = 2$  k $\Omega$ , unless otherwise noted.

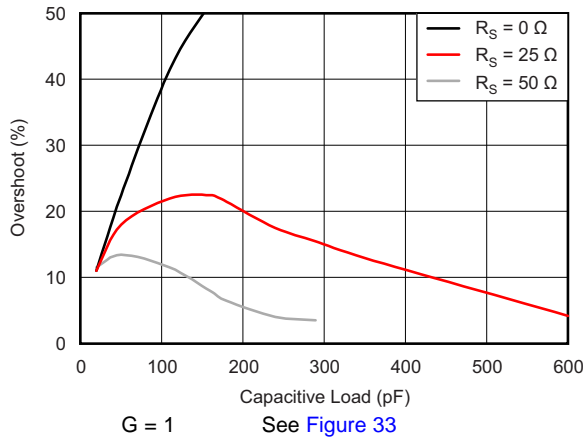


Figure 19. Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)

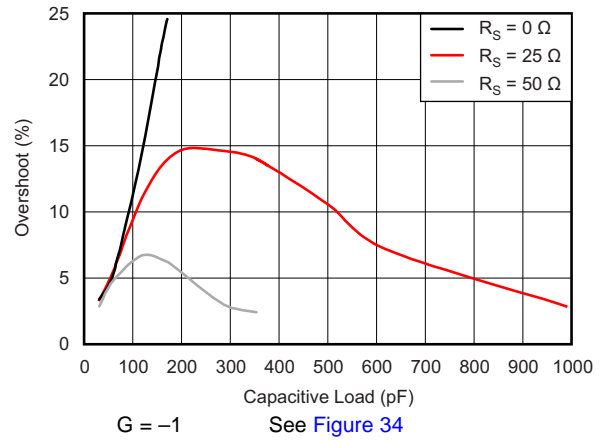


Figure 20. Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)

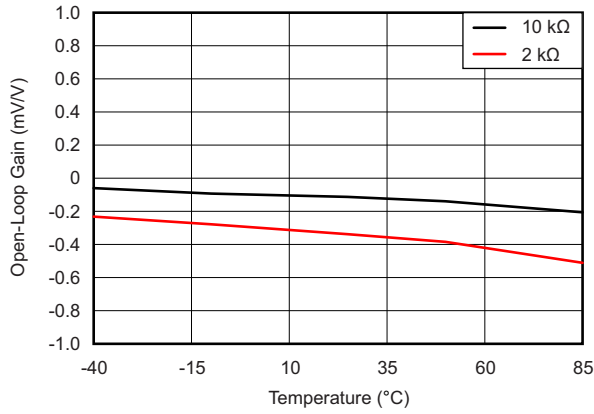


Figure 21. Open-Loop Gain vs Temperature

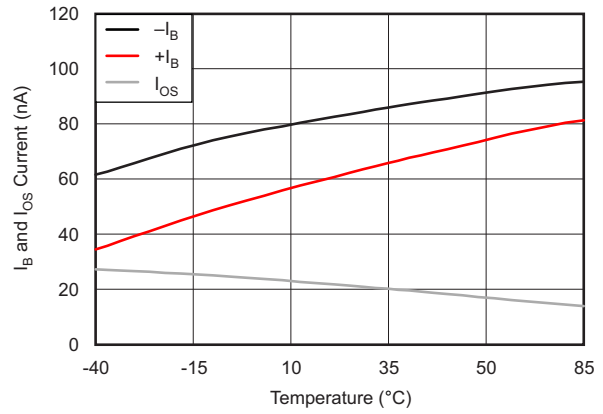


Figure 22.  $I_B$  and  $I_{OS}$  vs Temperature

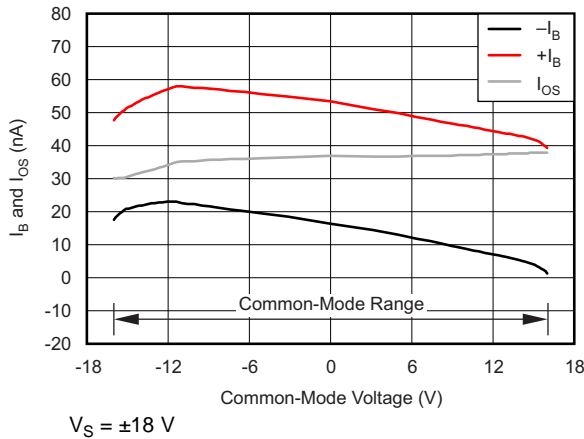


Figure 23.  $I_B$  and  $I_{OS}$  vs Common-Mode Voltage

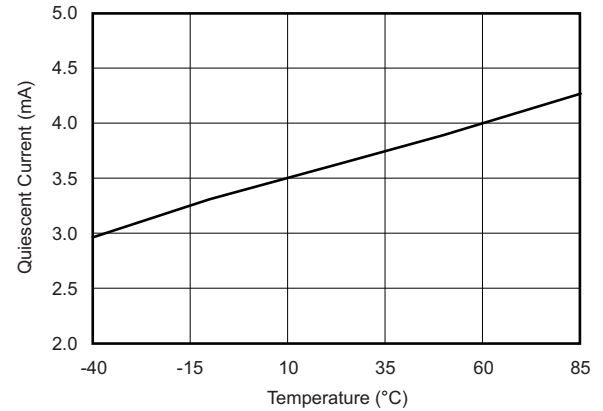


Figure 24. Quiescent Current vs Temperature

### Typical Characteristics (continued)

At  $T_A = 25^\circ$ ,  $V_S = \pm 15$  V, and  $R_L = 2$  k $\Omega$ , unless otherwise noted.

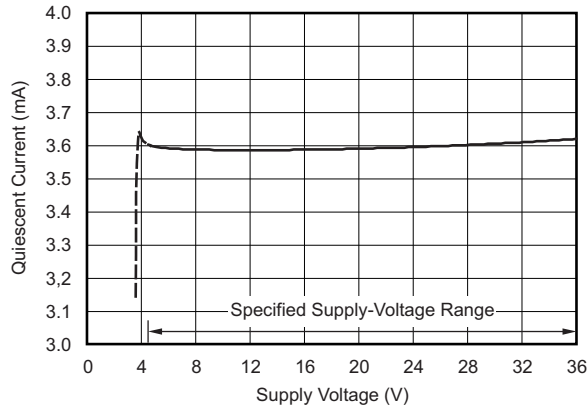


Figure 25. Quiescent Current vs Supply Voltage

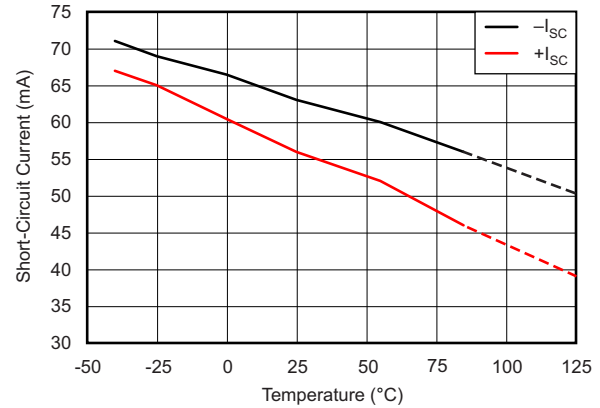


Figure 26. Short-Circuit Current vs Temperature

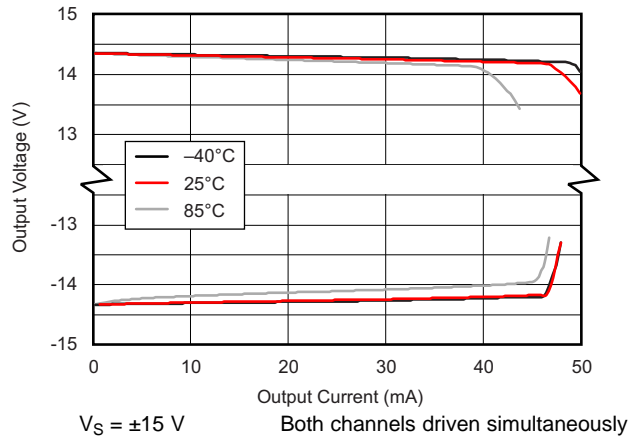


Figure 27. Output Voltage vs Output Current

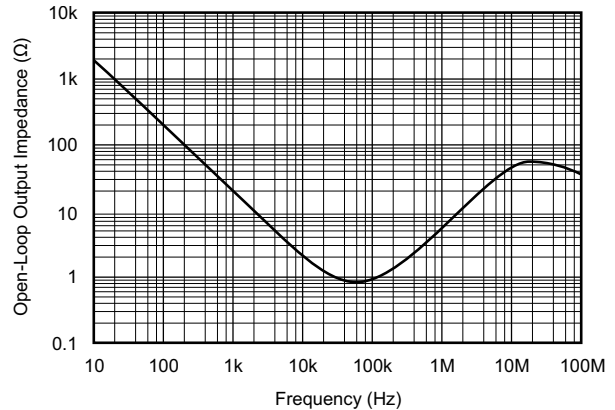


Figure 28. Open-Loop Output Impedance vs Frequency

## 7 Parameter Measurement Information

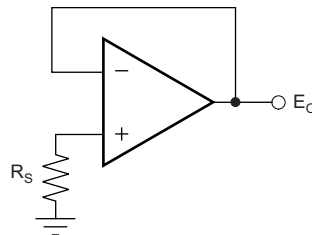
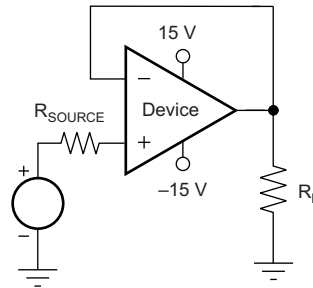
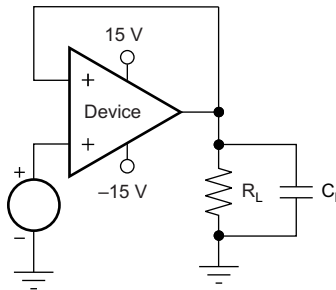
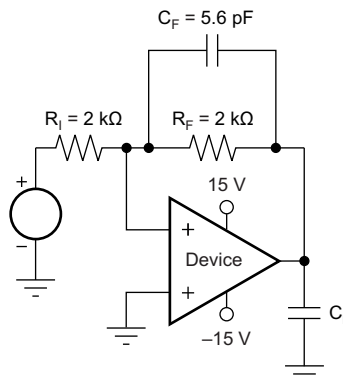
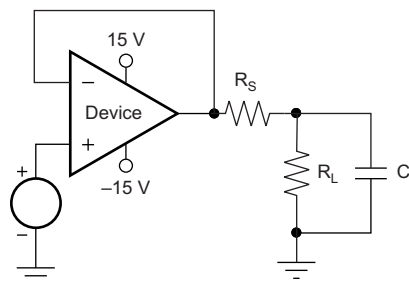
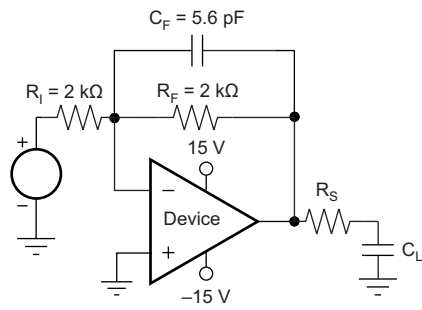


Figure 29. Circuit for Figure 3—Voltage Noise vs Source Resistance

**Parameter Measurement Information (continued)**

**Figure 30. Circuit for Figure 8 and Figure 10—THD+N Ratio vs Frequency**

**Figure 31. Circuit for Figure 15—Small-Signal Step Response (100 mV)**

**Figure 32. Circuit for Figure 16—Small-Signal Step Response (100 mV)**

**Figure 33. Circuit for Figure 19—Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)**

**Parameter Measurement Information (continued)**



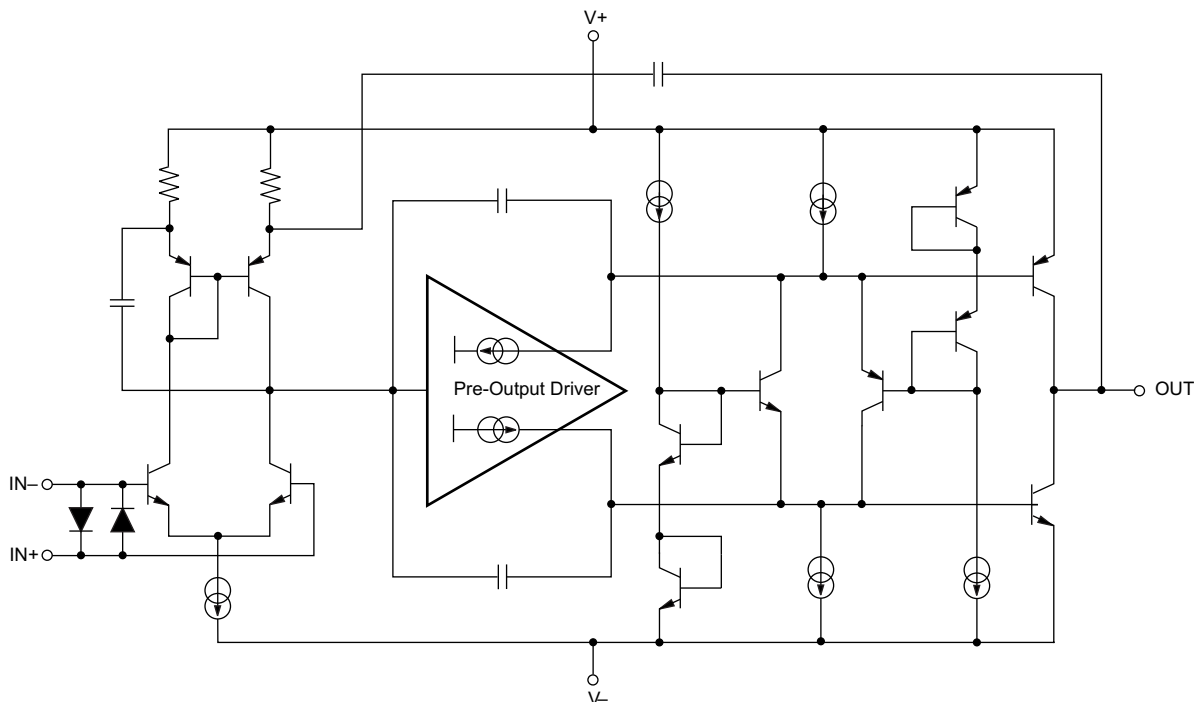
**Figure 34. Circuit for Figure 20—Small-Signal Overshoot vs Capacitive Load (100-mV Output Step)**

## 8 Detailed Description

### 8.1 Overview

The OPA1612-Q1 bipolar-input operational amplifier achieves very low  $1.1\text{-nV}/\sqrt{\text{Hz}}$  noise density with an ultralow distortion of 0.000015% at 1 kHz. The rail-to-rail output swing, within 600 mV with a 2-k $\Omega$  load, increases headroom and maximizes dynamic range. These devices also have a high output drive capability of  $\pm 40\text{ mA}$ . The wide supply range of  $\pm 2.25\text{ V}$  to  $\pm 18\text{ V}$ , on only 3.6 mA of supply current per channel, makes them applicable to both 5-V systems and 36-V audio applications. The OPA1612-Q1 op amp is unity-gain stable and provide excellent dynamic behavior over a wide range of load conditions.

### 8.2 Functional Block Diagram



### 8.3 Feature Description

#### 8.3.1 Power Dissipation

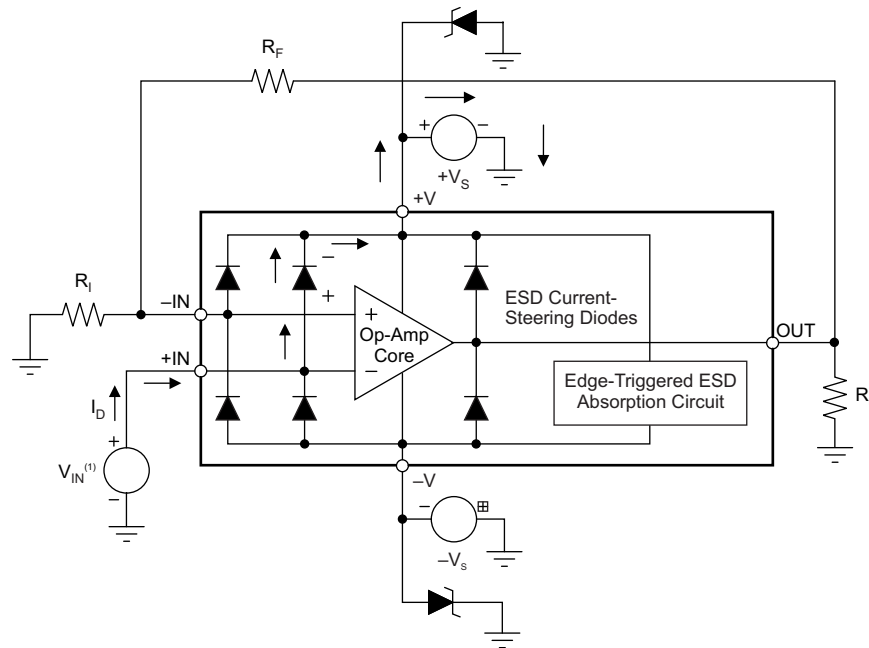
The OPA1612-Q1 op amp is capable of driving 2-k $\Omega$  loads with a power-supply voltage up to  $\pm 18\text{ V}$ . Internal power dissipation increases when operating at high supply voltages. Copper leadframe construction used in the OPA1612-Q1 op amp improves heat dissipation compared to conventional materials. Circuit board layout can also help minimize junction temperature rise. Wide copper traces help dissipate the heat by acting as an additional heat sink. Temperature rise can be further minimized by soldering the devices to the circuit board rather than using a socket.

#### 8.3.2 Electrical Overstress

Designers often ask questions about the capability of an operational amplifier to withstand electrical overstress. These questions tend to focus on the device inputs, but may involve the supply voltage pins or even the output pin. Each of these different pin functions have electrical stress limits determined by the voltage breakdown characteristics of the particular semiconductor fabrication process and specific circuits connected to the pin. Additionally, internal electrostatic discharge (ESD) protection is built into these circuits to protect them from accidental ESD events both before and during product assembly.

## Feature Description (continued)

Having a good understanding of this basic ESD circuitry and its relevance to an electrical overstress event is helpful. Figure 35 shows the ESD circuits contained in the OPA1612-Q1 device (indicated by the dashed line area). The ESD protection circuitry involves several current-steering diodes connected from the input and output pins and routed back to the internal power-supply lines, where they meet at an absorption device internal to the operational amplifier. This protection circuitry is intended to remain inactive during normal circuit operation.



(1)  $V_{IN} = +V_S + 500 \text{ mV}$ .

**Figure 35. Equivalent Internal ESD Circuitry and its Relation to a Typical Circuit Application**

An ESD event produces a short duration, high-voltage pulse that is transformed into a short duration, high-current pulse when discharged through a semiconductor device. The ESD protection circuits are designed to provide a current path around the operational amplifier core to prevent damage to the core. The energy absorbed by the protection circuitry is then dissipated as heat.

When an ESD voltage develops across two or more of the amplifier device pins, current flows through one or more of the steering diodes. Depending on the path that the current takes, the absorption device may activate. The absorption device internal to the OPA1612-Q1 device triggers when a fast ESD voltage pulse is impressed across the supply pins. Once triggered, the absorption device quickly activates and clamps the ESD pulse to a safe voltage level.

When the operational amplifier connects into a circuit such as the one Figure 35 shows, the ESD protection components are intended to remain inactive and not become involved in the application circuit operation. However, circumstances may arise where an applied voltage exceeds the operating voltage range of a given pin. If this condition occurs, some of the internal ESD protection circuits may possibly be biased on, and conduct current. Any such current flow occurs through steering diode paths and rarely involves the absorption device.

Figure 35 shows a specific example where the input voltage,  $V_{IN}$ , exceeds the positive supply voltage ( $+V_S$ ) by 500 mV or more. Much of what happens in the circuit depends on the supply characteristics. If  $+V_S$  can sink the current, one of the upper input steering diodes conducts and directs current to  $+V_S$ . Excessively high current levels can flow with increasingly higher  $V_{IN}$ . As a result, the datasheet specifications recommend that applications limit the input current to 10 mA.

## Feature Description (continued)

If the supply is not capable of sinking the current,  $V_{IN}$  may begin sourcing current to the operational amplifier, and then take over as the source of positive supply voltage. The danger in this case is that the voltage can rise to levels that exceed the operational amplifier absolute maximum ratings. In extreme but rare cases, the absorption device triggers on while  $+V_S$  and  $-V_S$  are applied. If this event happens, a direct current path is established between the  $+V_S$  and  $-V_S$  supplies. The power dissipation of the absorption device is quickly exceeded, and the extreme internal heating destroys the operational amplifier.

Another common question involves what happens to the amplifier if an input signal is applied to the input while the power supplies  $+V_S$  or  $-V_S$  are at 0 V. Again, the result depends on the supply characteristic while at 0 V, or at a level below the input signal amplitude. If the supplies appear as high impedance, then the operational amplifier supply current may be supplied by the input source via the current steering diodes. This state is not a normal bias condition; the amplifier most likely does not operate normally. If the supplies are low impedance, then the current through the steering diodes can become quite high. The current level depends on the ability of the input source to deliver current, and any resistance in the input path.

If there is an uncertainty about the ability of the supply to absorb this current, external zener diodes may be added to the supply pins; see [Figure 35](#). The zener voltage must be selected such that the diode does not turn on during normal operation. However, the zener diode voltage must be low enough so that the zener diode conducts if the supply pin begins to rise above the safe operating supply voltage level.

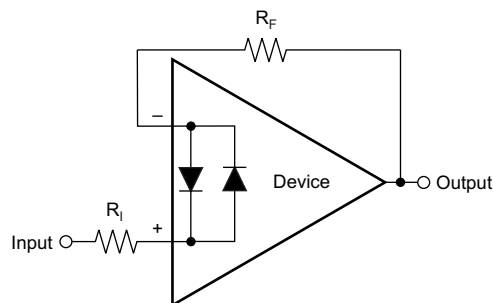
### 8.3.3 Operating Voltage

The OPA1612-Q1 op amp operates from  $\pm 2.25$ -V to  $\pm 18$ -V supplies while maintaining excellent performance. The OPA1612-Q1 device can operate with as little as +4.5 V between the supplies and with up to +36 V between the supplies. However, some applications do not require equal positive and negative output voltage swing. With the OPA1612-Q1 device, power-supply voltages do not need to be equal. For example, the positive supply could be set to +25 V with the negative supply at  $-5$  V.

In all cases, the common-mode voltage must be maintained within the specified range. In addition, key parameters are assured over the specified temperature range of  $T_A = -40^\circ\text{C}$  to  $+85^\circ\text{C}$ . Parameters that vary with operating voltage or temperature are shown in the [Typical Characteristics](#) section.

### 8.3.4 Input Protection

The input terminals of the OPA1612-Q1 device is protected from excessive differential voltage with back-to-back diodes, as [Figure 36](#) shows. In most circuit applications, the input protection circuitry has no consequence. However, in low-gain or  $G = +1$  circuits, fast ramping input signals can forward bias these diodes because the output of the amplifier cannot respond rapidly enough to the input ramp. This effect is illustrated in [Figure 17](#) of the [Typical Characteristics](#) section. If the input signal is fast enough to create this forward bias condition, the input signal current must be limited to 10 mA or less. If the input signal current is not inherently limited, an input series resistor ( $R_I$ ) or a feedback resistor ( $R_F$ ) can be used to limit the signal input current. This input series resistor degrades the low-noise performance of the OPA1612-Q1 device and is examined in the [Noise Performance](#) section. [Figure 36](#) shows an example configuration when both current-limiting input and feedback resistors are used.



**Figure 36. Pulsed Operation**



## 8.4 Device Functional Modes

The OPA1612-Q1 device has a single functional mode. The device is powered on as long as the power supply voltage is between 4.5 V ( $\pm 2.25$  V) and 36 V ( $\pm 18$  V).

## 9 Application and Implementation

### NOTE

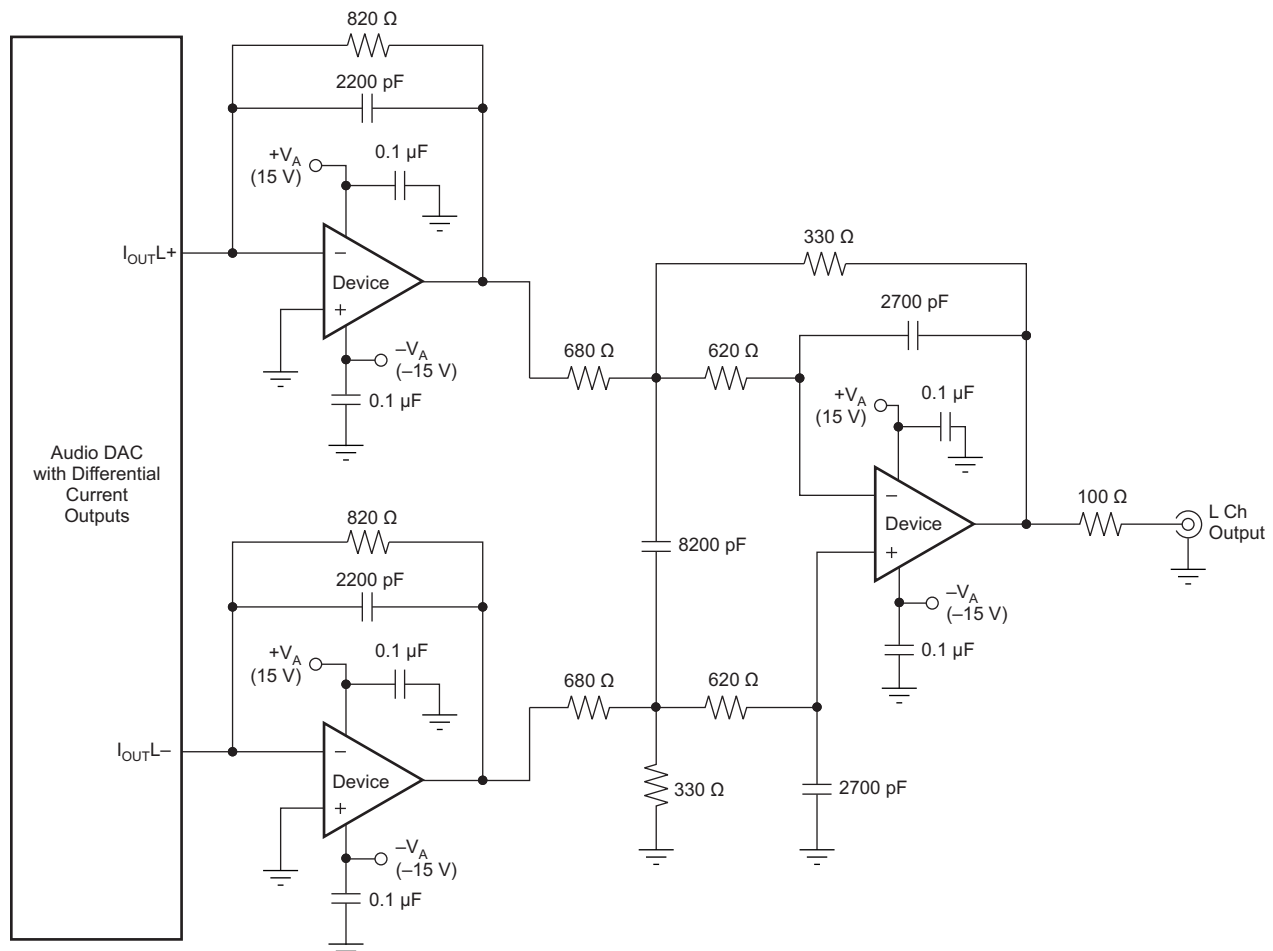
Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

### 9.1 Application Information

The OPA1612-Q1 device is unity-gain stable, precision op amp with very low noise; these devices are also free from output phase reversal. Applications with noisy or high-impedance power supplies require decoupling capacitors close to the device power-supply pins. In most cases, 0.1- $\mu\text{F}$  capacitors are adequate.

### 9.2 Typical Application

Figure 37 shows how to use the OPA1612-Q1 device as an amplifier for professional audio headphones. The circuit shows the left side stereo channel. An identical circuit is used to drive the right side stereo channel.



**Figure 37. Audio DAC Post Filter (I/V Converter and Low-Pass Filter)**

## Typical Application (continued)

### 9.2.1 Design Requirements

Use [Equation 1](#) to calculate the total circuit noise.

$$E_o^2 = e_n^2 + (i_n R_s)^2 + 4kTR_s$$

where

- $e_n$  = voltage noise
- $i_n$  = current noise
- $R_s$  = source impedance
- $k$  = Boltzmann's constant =  $1.38 \times 10^{-23}$  J/K
- $T$  = temperature in degrees Kelvin (K)

(1)

### 9.2.2 Detailed Design Procedure

#### 9.2.2.1 Noise Performance

[Figure 40](#) shows the total circuit noise for varying source impedances with the op amp in a unity-gain configuration (no feedback resistor network, and therefore no additional noise contributions).

The OPA1612-Q1 device (GBW = 40 MHz, G = +1) is shown with total circuit noise calculated. The op amp contributes both a voltage noise component and a current noise component. The voltage noise is commonly modeled as a time-varying component of the offset voltage. The current noise is modeled as the time-varying component of the input bias current and reacts with the source resistance to create a voltage component of noise. Therefore, the lowest noise op amp for a given application depends on the source impedance. For low source impedance, current noise is negligible, and voltage noise generally dominates. The low voltage noise of the OPA1612-Q1 device makes it a good choice for use in applications where the source impedance is less than 1 k $\Omega$ .

##### 9.2.2.1.1 Basic Noise Calculations

Design of low-noise op amp circuits requires careful consideration of a variety of possible noise contributors: noise from the signal source, noise generated in the op amp, and noise from the feedback network resistors. The total noise of the circuit is the root-sum-square combination of all noise components.

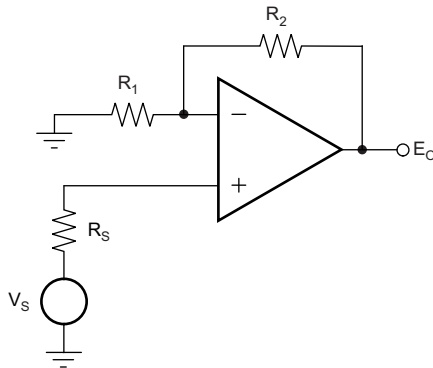
The resistive portion of the source impedance produces thermal noise proportional to the square root of the resistance. [Figure 40](#) plots this function. The source impedance is usually fixed; consequently, select the op amp and the feedback resistors to minimize the respective contributions to the total noise.

[Figure 38](#) shows both inverting and noninverting op amp circuit configurations with gain. In circuit configurations with gain, the feedback network resistors also contribute noise.

The current noise of the op amp reacts with the feedback resistors to create additional noise components. The feedback resistor values can generally be chosen to make these noise sources negligible. The equations for total noise are shown for both configurations.

**Typical Application (continued)**

Noise in Noninverting Gain Configuration



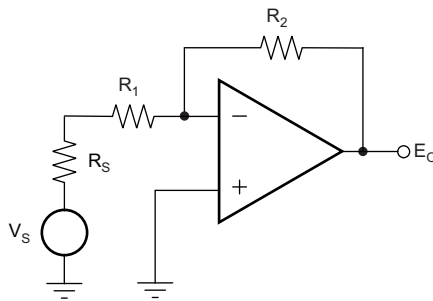
Noise at the output:

$$E_O^2 = \left[ 1 + \frac{R_2}{R_1} \right]^2 e_n^2 + e_1^2 + e_2^2 + (i_n R_2)^2 + e_S^2 + (i_n R_S)^2 \left[ 1 + \frac{R_2}{R_1} \right]^2$$

where

- $e_S = \sqrt{4kTR_S} \times \left[ 1 + \frac{R_2}{R_1} \right]$  = thermal noise of  $R_S$
- $e_1 = \sqrt{4kTR_1} \times \left[ \frac{R_2}{R_1} \right]$  = thermal noise of  $R_1$
- $e_2 = \sqrt{4kTR_2}$  = thermal noise of  $R_2$

Noise in Inverting Gain Configuration



Noise at the output:

$$E_O^2 = \left[ 1 + \frac{R_2}{R_1 + R_S} \right]^2 e_n^2 + e_1^2 + e_2^2 + (i_n R_2)^2 + e_S^2$$

where

- $e_S = \sqrt{4kTR_S} \times \left[ \frac{R_2}{R_1 + R_S} \right]$  = thermal noise of  $R_S$
- $e_1 = \sqrt{4kTR_1} \times \left[ \frac{R_2}{R_1 + R_S} \right]$  = thermal noise of  $R_1$
- $e_2 = \sqrt{4kTR_2}$  = thermal noise of  $R_2$

At 1 kHz,  $e_n = 1.1 \text{ nV}/\sqrt{\text{Hz}}$  and  $i_n = 1.7 \text{ pA}/\sqrt{\text{Hz}}$ .

**Figure 38. Noise Calculation in Gain Configurations**

**9.2.2.2 Total Harmonic Distortion Measurements**

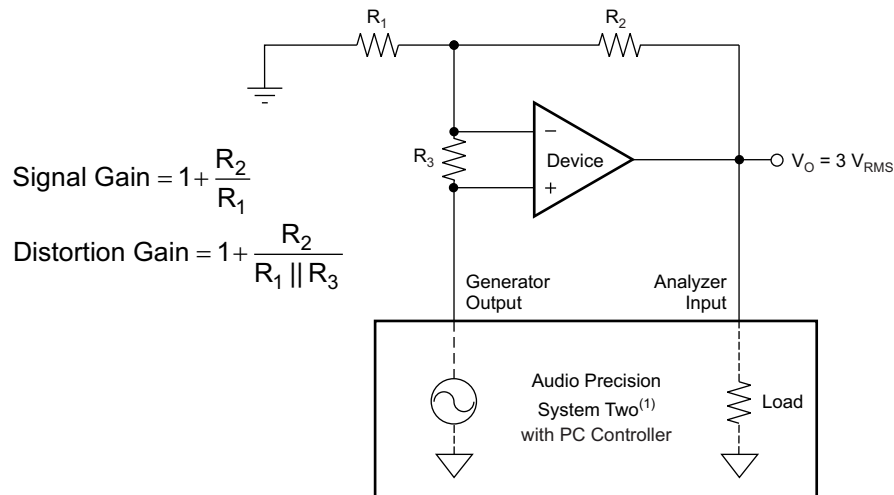
The OPA1612-Q1 op amp has excellent distortion characteristics. THD + noise is below 0.00008% ( $G = +1$ ,  $V_O = 3 V_{RMS}$ ,  $BW = 80 \text{ kHz}$ ) throughout the audio frequency range, 20 Hz to 20 kHz, with a 2-k $\Omega$  load (see [Figure 7](#) for characteristic performance).

The distortion produced by OPA1612-Q1 op amp is below the measurement limit of many commercially available distortion analyzers. However, a special test circuit (such as [Figure 39](#) shows) can be used to extend the measurement capabilities.

Op amp distortion can be considered an internal error source that can be referred to the input. [Figure 39](#) shows a circuit that causes the op amp distortion to be 101 times (or approximately 40 dB) greater than that normally produced by the op amp. The addition of  $R_3$  to the otherwise standard noninverting amplifier configuration alters the feedback factor or noise gain of the circuit. The closed-loop gain is unchanged, but the feedback available for error correction is reduced by a factor of 101, thus extending the resolution by 101. Note that the input signal and load applied to the op amp are the same as with conventional feedback without  $R_3$ . Keep the value of  $R_3$  small to minimize its effect on the distortion measurements.

**Typical Application (continued)**

Validity of this technique can be verified by duplicating measurements at high gain and/or high frequency where the distortion is within the measurement capability of the test equipment. Measurements for this data sheet were made with an audio precision system two distortion and noise analyzer, which greatly simplifies such repetitive measurements. The measurement technique can, however, be performed with manual distortion measurement instruments.



(1) For measurement bandwidth, see [Figure 7](#) through [Figure 12](#).

SIGNAL GAIN	DISTORTION GAIN	R <sub>1</sub>	R <sub>2</sub>	R <sub>3</sub>
1	101	∞	1 kΩ	10 Ω
-1	101	4.99 kΩ	4.99 kΩ	49.9 kΩ
10	110	549 Ω	4.99 kΩ	49.9 kΩ

**Figure 39. Distortion Test Circuit**

**9.2.2.3 Capacitive Loads**

The dynamic characteristics of the OPA1612-Q1 device is optimized for commonly encountered gains, loads, and operating conditions. The combination of low closed-loop gain and high capacitive loads decreases the phase margin of the amplifier and can lead to gain peaking or oscillations. As a result, heavier capacitive loads must be isolated from the output. The simplest way to achieve this isolation is to add a small resistor (R<sub>S</sub> equal to 50 Ω, for example) in series with the output.

This small series resistor also prevents excess power dissipation if the output of the device becomes shorted. [Figure 19](#) and [Figure 20](#) illustrate graphs of *Small-Signal Overshoot vs Capacitive Load* for several values of R<sub>S</sub>. For details of analysis techniques and application circuits, refer to Applications Bulletin AB-028, *Feedback Plots Define Op Amp AC Performance* ([SBOA015](#)).

## Typical Application (continued)

### 9.2.3 Application Curves

Equation 1 applies to Figure 40 and Figure 41.

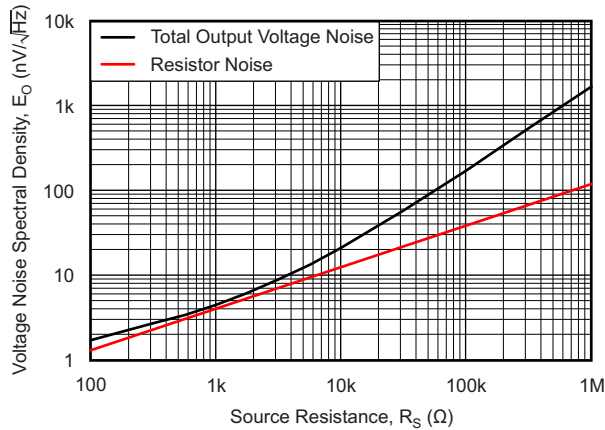


Figure 40. Noise Performance of the OPA1612-Q1 in Unity-Gain Buffer Configuration

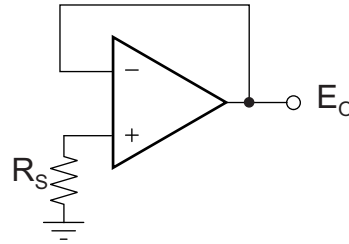


Figure 41. Circuit for Figure 40

## 10 Power-Supply Recommendations

The OPA1612-Q1 device is specified for operation from 4.5 V to 36 V ( $\pm 2.25$  V to  $\pm 18$  V); many specifications apply from  $-40^{\circ}\text{C}$  to  $+85^{\circ}\text{C}$ . Parameters that can exhibit significant variance with regard to operating voltage or temperature are presented in the *Typical Characteristics* section.

### CAUTION

Supply voltages larger than 40 V can permanently damage the device; see the *Absolute Maximum Ratings* table.

Place 0.1- $\mu\text{F}$  bypass capacitors close to the power-supply pins to reduce errors coupling in from noisy or high-impedance power supplies. For more detailed information on bypass capacitor placement, refer to the *Layout* section.

## 11 Layout

### 11.1 Layout Guidelines

For best operational performance of the device, use good printed circuit board (PCB) layout practices, including:

- Noise can propagate into analog circuitry through the power pins of the circuit as a whole and the op amp itself. Bypass capacitors are used to reduce the coupled noise by providing low-impedance power sources local to the analog circuitry.
  - Connect low-ESR, 0.1- $\mu\text{F}$  ceramic bypass capacitors between each supply pin and ground, placed as close to the device as possible. A single bypass capacitor from V+ to ground is applicable for single-supply applications.
- Separate grounding for analog and digital portions of the circuitry is one of the simplest and most-effective methods of noise suppression. One or more layers on multilayer PCBs are usually devoted to ground planes. A ground plane helps distribute heat and reduces EMI noise pickup. Make sure to physically separate digital and analog grounds while paying attention to the flow of the ground current. For more detailed information, refer to the application report, *Circuit Board Layout Techniques* (SLOA089).
- In order to reduce parasitic coupling, run the input traces as far away from the supply or output traces as possible. If these traces cannot be keep them separate, crossing the sensitive trace perpendicular as

## Layout Guidelines (continued)

- opposed to in parallel with the noisy trace is the preferred method.
- Place the external components as close to the device as possible. As shown in Figure 42, keeping RF and RG close to the inverting input minimizes parasitic capacitance.
- Keep the length of input traces as short as possible. Always remember that the input traces are the most sensitive part of the circuit.
- Consider a driven, low-impedance guard ring around the critical traces. A guard ring can significantly reduce leakage currents from nearby traces that are at different potentials.

## 11.2 Layout Example

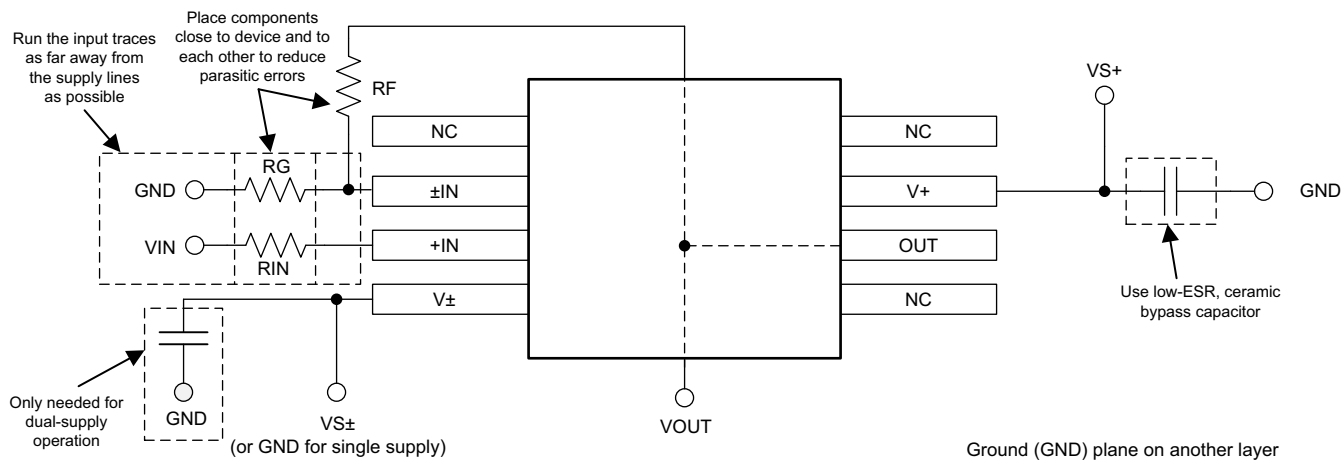
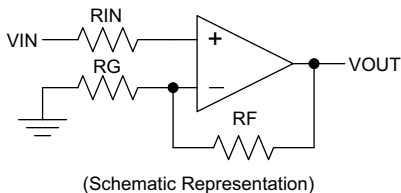


Figure 42. Operational Amplifier Board Layout for a Noninverting Configuration

## 12 Device and Documentation Support

### 12.1 Documentation Support

#### 12.1.1 Related Documentation

For related documentation see the following:

- *Feedback Plots Define Op Amp AC Performance* , [SBOA015](#)
- *Circuit Board Layout Techniques*, [SLOA089](#)

### 12.2 Community Resource

The following links connect to TI community resources. Linked contents are provided "AS IS" by the respective contributors. They do not constitute TI specifications and do not necessarily reflect TI's views; see TI's [Terms of Use](#).

**TI E2E™ Online Community** *TI's Engineer-to-Engineer (E2E) Community*. Created to foster collaboration among engineers. At [e2e.ti.com](http://e2e.ti.com), you can ask questions, share knowledge, explore ideas and help solve problems with fellow engineers.

**Design Support** *TI's Design Support* Quickly find helpful E2E forums along with design support tools and contact information for technical support.

### 12.3 Trademarks

E2E is a trademark of Texas Instruments.

SoundPlus is a trademark of Texas Instruments, Inc.

All other trademarks are the property of their respective owners.

### 12.4 Electrostatic Discharge Caution



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

### 12.5 Glossary

[SLYZ022](#) — *TI Glossary*.


This glossary lists and explains terms, acronyms, and definitions.

## 13 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.



**PACKAGING INFORMATION**

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
OPA1612AQDRQ1	ACTIVE	SOIC	D	8	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	1612Q1	

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSELETE:** TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

**TBD:** The Pb-Free/Green conversion plan has not been defined.

**Pb-Free (RoHS):** TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

**Pb-Free (RoHS Exempt):** This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

**Green (RoHS & no Sb/Br):** TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "-" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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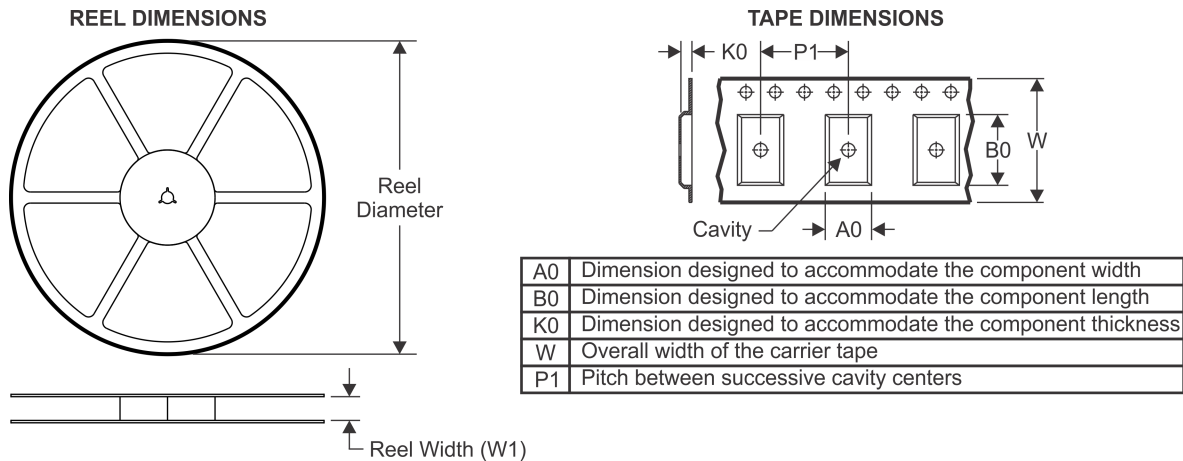
In no event shall TI's liability arising out of such information exceed the total purchase price of the TI part(s) at issue in this document sold by TI to Customer on an annual basis.

**OTHER QUALIFIED VERSIONS OF OPA1612-Q1 :**

- Catalog: [OPA1612](#)

## NOTE: Qualified Version Definitions:

- Catalog - TI's standard catalog product

**TAPE AND REEL INFORMATION**

**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
OPA1612AQDRQ1	SOIC	D	8	2500	330.0	12.4	6.4	5.2	2.1	8.0	12.0	Q1

TAPE AND REEL BOX DIMENSIONS



\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
OPA1612AQDRQ1	SOIC	D	8	2500	367.0	367.0	35.0

D (R-PDSO-G8)

PLASTIC SMALL OUTLINE



- NOTES:
- A. All linear dimensions are in inches (millimeters).
  - B. This drawing is subject to change without notice.
  - $\triangle C$  Body length does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.006 (0,15) each side.
  - $\triangle D$  Body width does not include interlead flash. Interlead flash shall not exceed 0.017 (0,43) each side.
  - E. Reference JEDEC MS-012 variation AA.

D (R-PDSO-G8)

PLASTIC SMALL OUTLINE



- NOTES:
- All linear dimensions are in millimeters.
  - This drawing is subject to change without notice.
  - Publication IPC-7351 is recommended for alternate designs.
  - Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Refer to IPC-7525 for other stencil recommendations.
  - Customers should contact their board fabrication site for solder mask tolerances between and around signal pads.

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